CHEAP MICROWAVE FILTERS

By Kent Britain, WA5VJB

These filters are for our 3, 5 and 10 GHz ham bands. The design is based on the filters used in the DJ6EP 5760 MHz transverter.

When I first saw these filters used in the DJ6EP transverter I thought; Wow, how neat and simple! But Roman's design used Teflon P.C. board and small pins through 50 Ohm stripline for coupling. The next trick was to find a simple way of putting them together with commonly available materials. I ended up using 1/2", 3/4", and 1" Copper plumbing end caps sweat soldered onto common PC board.

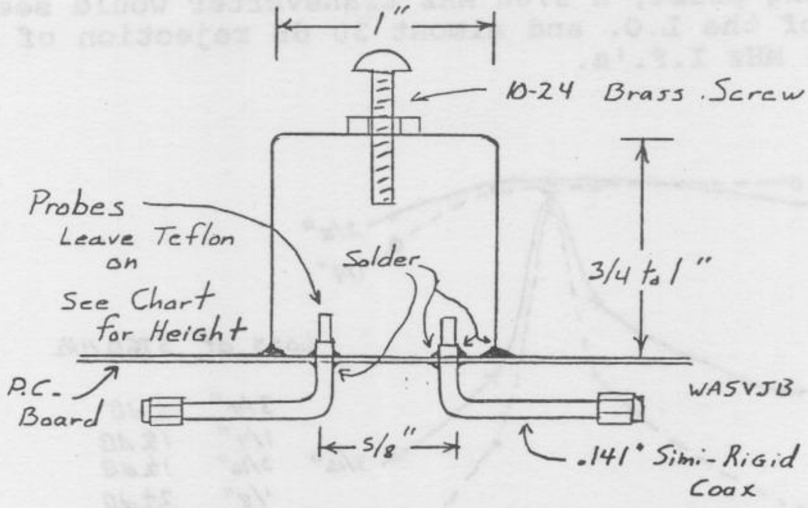
First I've built a bunch of these filters, and they all worked. Next I built several with intentional errors, lots of sloppy solder, misaligned probes, unequal probes, off center tuning screws, etc. Loss went up a bit on a few of them, but they all WORKED! These guys are very forgiving!

The length of the probe determines the coupling and therefore the Q of the filter. Keep the probes as short as you can, consistent with how much loss you can stand in your system. I did build some multi-stage versions to get a tighter bandwidth. But it really wasn't worth effort, just use shorter probes.

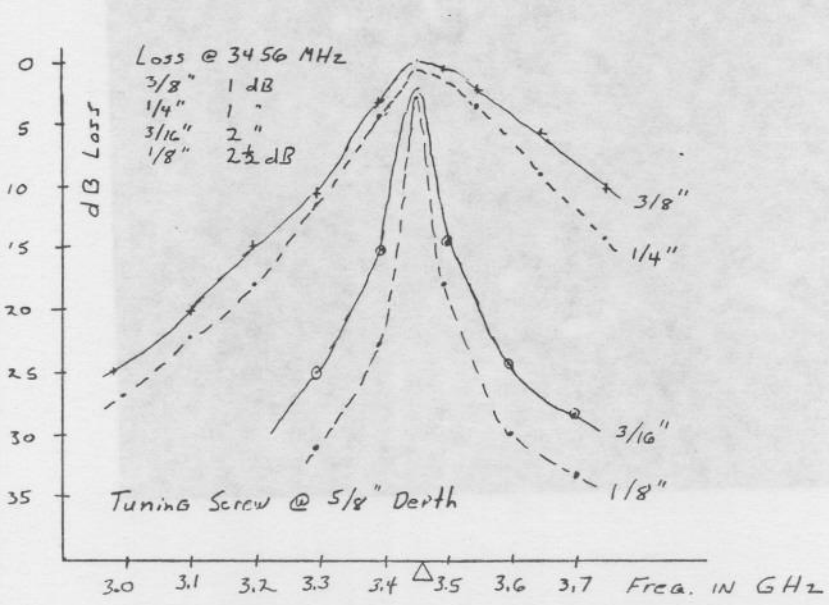
You can drill and tap the hole for the tuning screw, but I found it much easier to drill a slightly undersized hole and just force a steel screw (same thread size) through. The locking nut is tightened down after you have everything tuned.

3456 MHz Filter

The 3456 MHz version is based on a 1" Copper plumbing end cap. The hollow filter resonates between 6 and 7 GHz. The tuning screw pulls the filter down to 3.4 GHz at a depth of about 5/8".



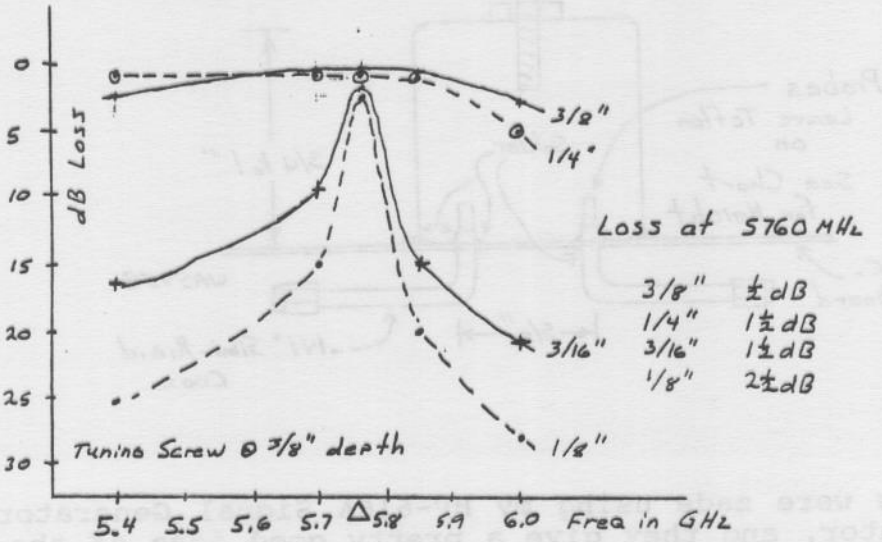
These plots were made using my HP-616A Signal Generator and HP-415B indicator, and they give a pretty good idea of the shape of these filters. In a 3456 MHz station using a 144 MHz I.F., a filter using 3/16" probes would give 25 dB rejection of the L.O. and better than 30 dB rejection of the image with 2 dB of loss.

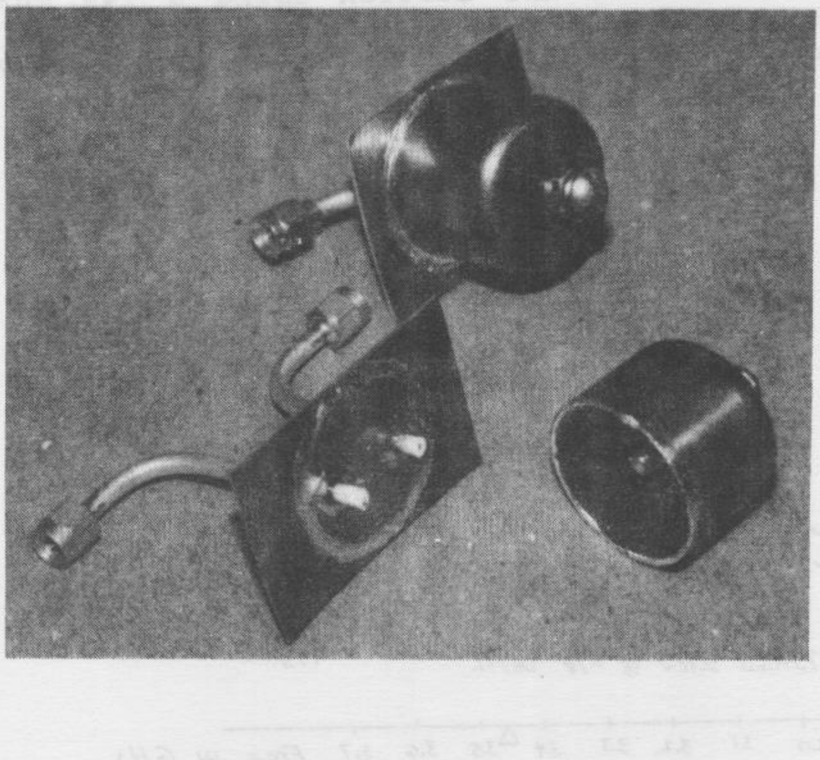


5760 MHz 1" Filter

The 1" filters will also tune 5760 MHz with the tuning screw set at about 3/8" into the cavity. The plots below were made using my HP-614A signal generator driving a passive tripler and bandpass filter into a HP-415B indicator. Again a pretty good idea of the characteristics of these filters emerge.

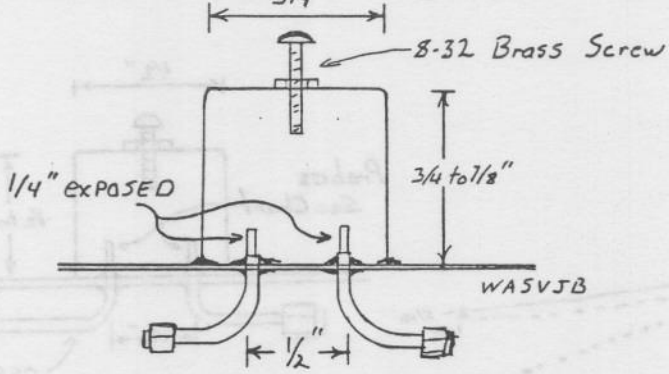
With a 1/8" long probe, a 5760 MHz transverter would see about 20 dB rejection of the L.O. and almost 30 dB rejection of the image when using 144 MHz I.F.'s.

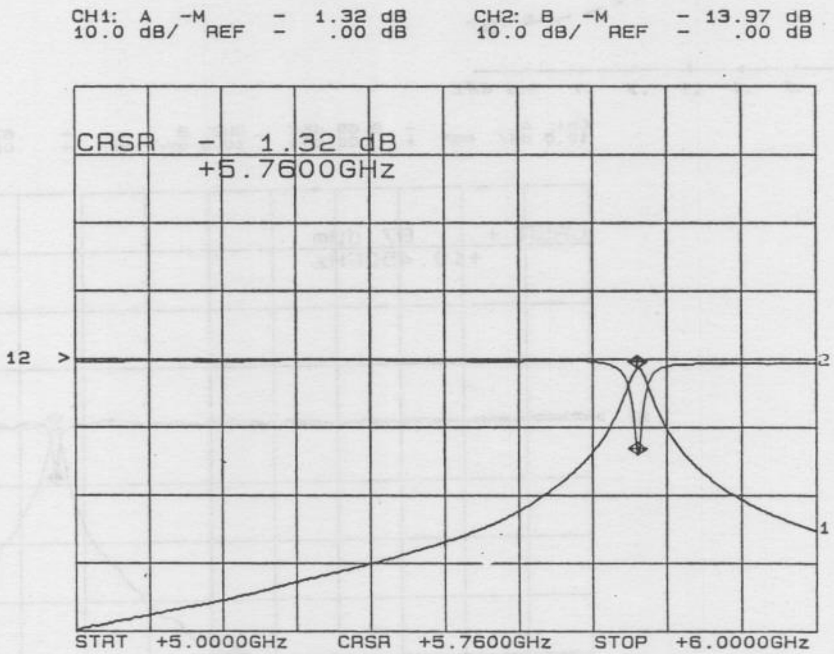




5760 MHz 3/4" Filter

This was one of the filters I was fortunate to get plotted on some really fancy equipment. I didn't get an opportunity to build a family of these filters before the proceedings deadline, but my first try seems to have done pretty well. Again a 5760 MHz transverter using a 144 MHz I.F. would have about 20 dB rejection of the L.O. and almost 30 dB image rejection with less insertion loss than the 1" filter.

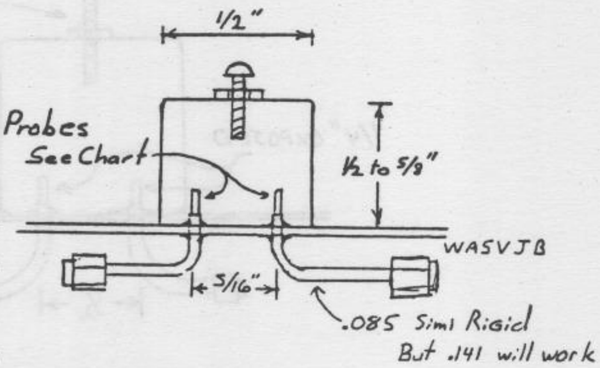


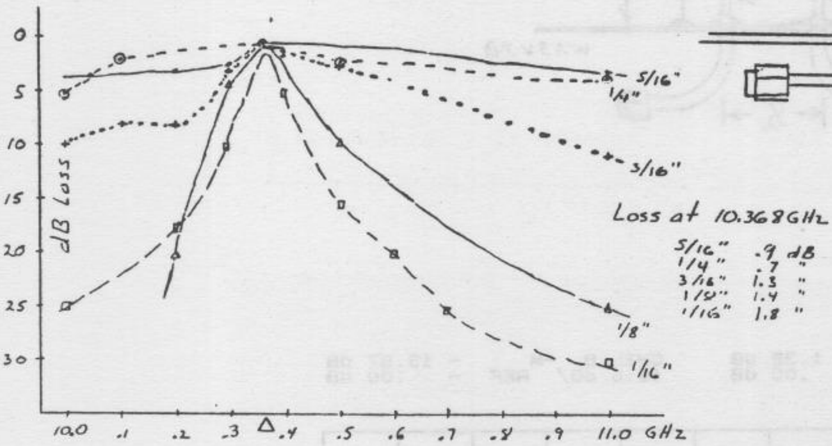


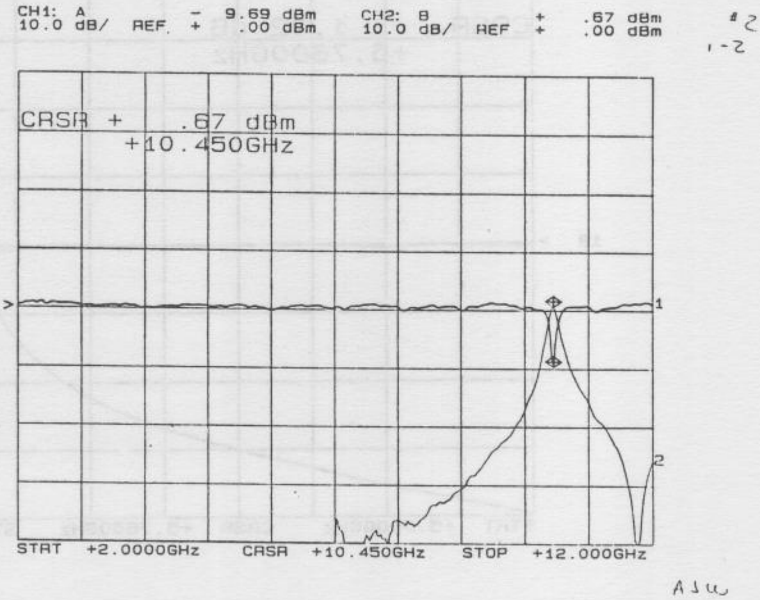
10 GHz Filter

When I first started building these probe coupled filters, they were used at 10.368 GHz. If you can dig up some .085" semi-rigid coax, it's much easier to use than the larger .141", but both sizes work. The filter resonates somewhere between 11.5 and 12GHz, so while digging through the bins at your hardware store, look for the longer end caps. The longer ones will have slightly lower loss, but it's not worth driving around town. I did try replacing the brass tuning screw with a steel screw on the 1/8" filter, loss went up from 1.3 to 2.0 dB.

The fancy plot shows a filter plotted from 2 to 12 GHz.





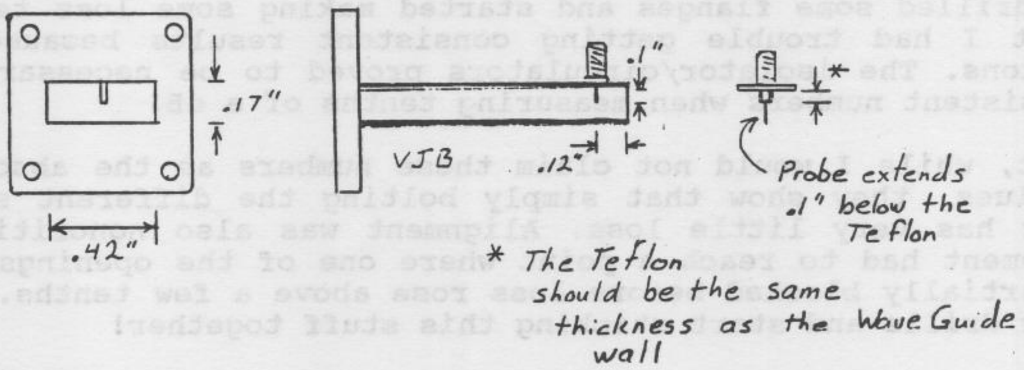


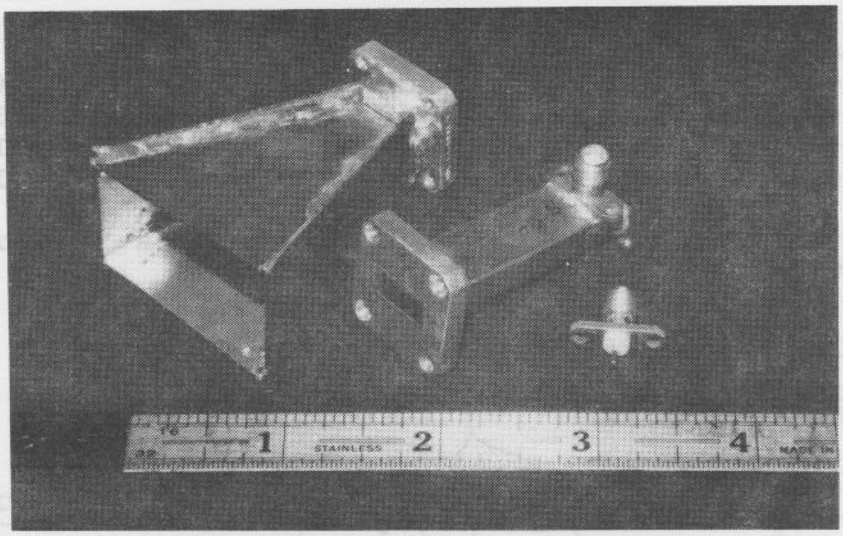
24.1 GHz Transition

When I first started some serious work with 24 GHz, one of the first items I needed was a WaveGuide to Coax transition. Very few of the commercial K band transitions are designed for use near our 24 GHz ham band so I came up with this design optimized for 24.1 GHz.

In constructing this transitions you must use either K or SMA connectors. I highly suggest the 2 hold flange mounts and avoid the stainless steel SMA's which are impossible to solder. It can be a bit tricky to solder the SMA and the backplate at the same time so use plenty of clamps or a vice. My thanks to K5SXK for his help with the "Wavelength in Guide" calculations.

WR-42 / WG-20 to SMA





WAVEGUIDE TRANSITIONS

by Kent Britain, WA5VJB

In putting together several 10 GHz stations out of surplus parts, the first thing you notice is the different sizes of moding, WR112, WR 90, WR 75, and WR 62. These can be identified by measuring the width of the opening. WR112 is 1.12", WR 90 is .9", WR 75 is .75" and of course WR 62 is .62" across.

Well, very quickly you'd like to hook a WR 90 thinga-migag, to a WR 75 whatsamacallit. I had two commercial adapters and they had simply milled a step changing the opening from one waveguide size to another. I contacted our local waveguide expert (K5SXK) and asked Harold what was going on. He explained that the impedance of a waveguide is the ratio of width to height, so if you go from one size to another it's like connecting RG 8 to RG 58.

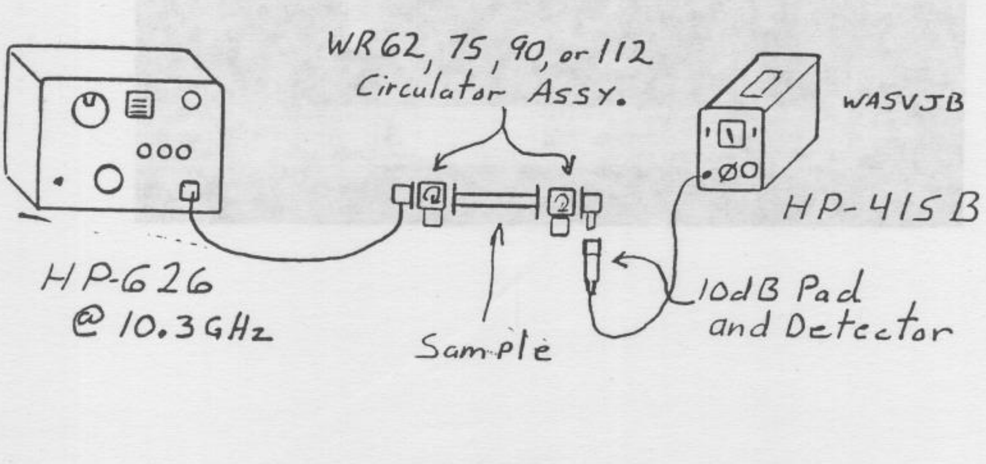
So I redrilled some flanges and started making some loss tests. At first I had trouble getting consistent results because of reflections. The isolator/circulators proved to be necessary to get consistent numbers when measuring tenths of a dB.

In short, while I would not claim these numbers as the absolute loss values, they show that simply bolting the different sizes together has very little loss. Alignment was also noncritical. Misalignment had to reach a point where one of the openings was being partially blocked before loss rose above a few tenths. Get out your drills and start sticking this stuff together!

Results:

Flange	Sample WR-62	WR-75	WR-90	WR-112	
WR-62	>.1dB	.3dB	.3dB	.4dB	(dB Loss)
WR-75	.3dB	>.1dB	.1dB	.1dB	
WR-90	.3dB	.1dB	>.1dB	>.1dB	
WR-112	.4dB	.2dB	.1dB	>.1dB	

Note: This test is actually measuring the loss in two waveguide size transitions.



Pipe-Cap Filters Revisited

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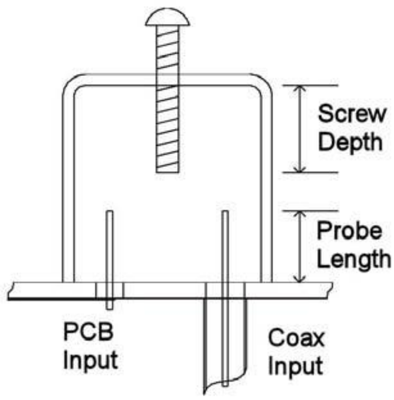
Pipe-cap filters have been used in amateur microwave equipment for at least 20 years, but are still not well understood, and design information is lacking. WA5VJB[1] borrowed the idea from a transverter by DJ6EP and DC0DA[2] and published some measured data which was enough to get others started. I used ½" pipe-cap filters in a 10 GHz mixer[3] and ¾" pipe-cap filters in a 5760 MHz mixer[4,5], but my implementations were cut-and-try. I later expanded these mixers into single-board transverters: one[6] for 5760 with five pipe-caps, and then one[7] for 10.368 GHz with seven ½" pipe-cap filters plus two ¾" caps in the LO chain. The number of filters was needed to get adequate selectivity on both transmit and receive without excessive filter loss, plus some margin to allow for reproducibility, since neither the selectivity nor the loss was well quantified. Both single-board transverters have been improved by Down-East Microwave[8] and made available in kit or finished form. The DB6NT[9] 10 GHz transverter uses a similar style of filter.

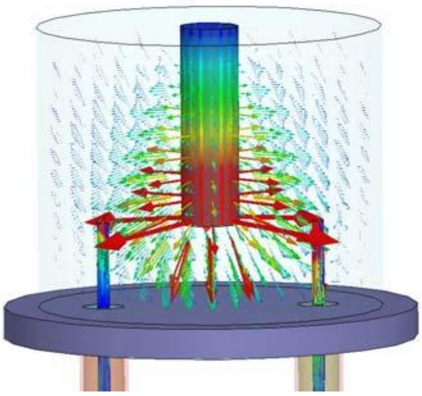
Pipe-Cap Resonators

Figure 1



The usual configuration for a pipe-cap filter is sketched in Figure 1: a metal plate shorting the open end, with probes for input and output, and a central tuning screw through the top of the cap. Two varieties of probe are shown in the figure. There has been some speculation about various cavity modes operating in these filters, but simulation with electromagnetic software, Ansoft **HFSS**[10], shows the electric field configuration with a tuning screw, seen in Figure 2. The pipe-cap filter is a simple coaxial quarter-wave resonator (which hams often call a cavity). The tuning screw acts as the coax center conductor, with a radial electric field around it; the field intensity increases toward the open end of the screw. The resonant frequency is determined by the inserted length of the screw; Figure 3 shows that the same screw length produces the same resonant frequency in three different sizes of pipe caps. The other dimensions do not affect the frequency, as they would if a waveguide cavity mode were involved.

Figure 2



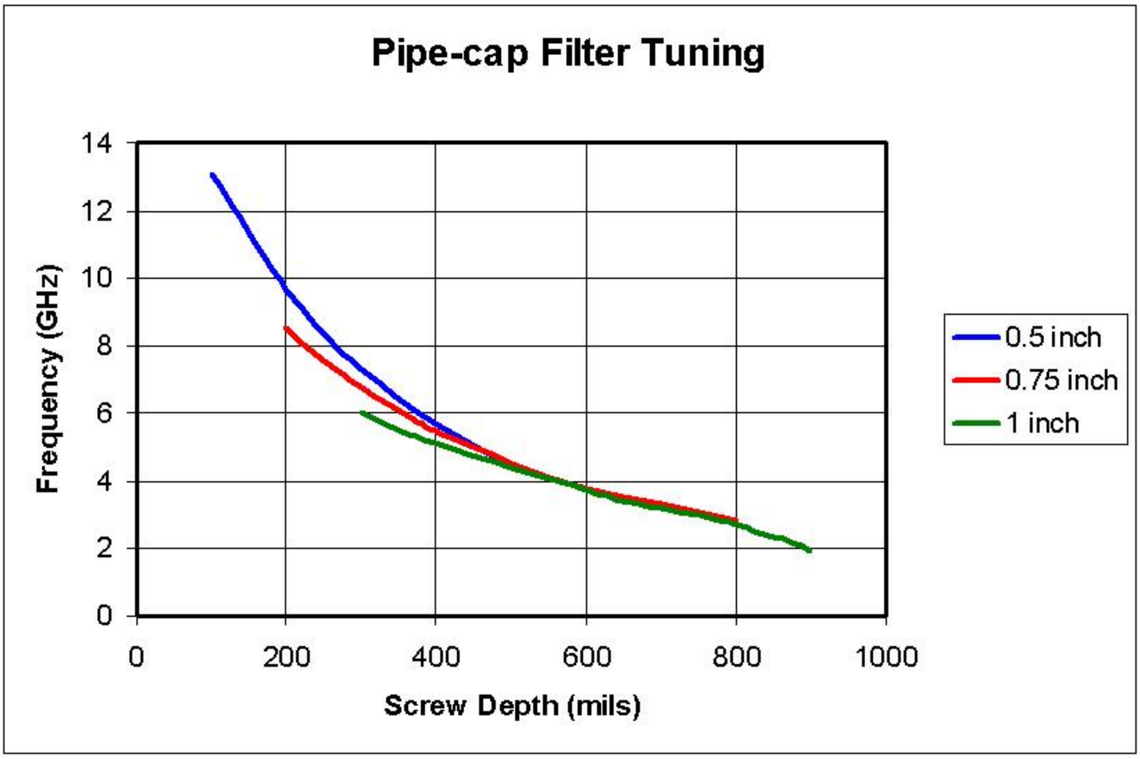


Figure 3

With the screw completely removed, true cavity modes may be found. These produce resonances at frequencies higher than those normally used for a given size cap, and probably set the upper frequency limit for a given size. For instance, a one-inch pipe cap (nominal plumbing size, to fit over copper tubing with a one inch inner diameter) with no screw resonates at 7.923 GHz, measured for two different heights of pipe cap – the height has no effect on this resonance, only the diameter. Normal use for this size pipe-cap would be below 5 GHz.

The input and output probes couple to the open end of the quarter-wave resonator, the tuning screw, so they are providing predominantly capacitive coupling. Magnetic coupling could also be used, for instance, a loop at the shorted end of the quarter-wave, but it would be more difficult to assemble and adjust.

Since the open end of the screw moves with frequency, the probe coupling also varies with frequency. Increased coupling loads the resonator, increasing the bandwidth. The equivalent circuit of a quarter-wave resonator is simply a parallel-tuned circuit, shown in Figure 4. Resonator losses are lumped into an equivalent resistance, **Ro**, in parallel with the tuned circuit. The resonator has an unloaded $\boldsymbol{Q}$, $\boldsymbol{Q}_U = \mathbf{Ro} / \mathbf{X_{Lo}}$ where $\mathbf{X_{Lo}}$ is the reactance of the inductor. For a high-$\boldsymbol{Q}$ resonator, **Ro** is a very high resistance.

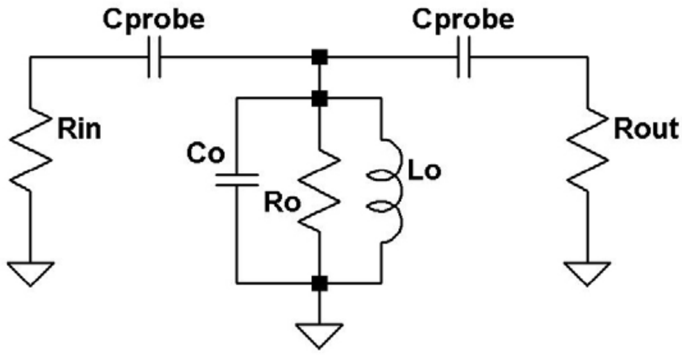


Figure 4. Pipe-cap resonator equivalent circuit

In most RF circuits, **Rin** and **Rout** are 50 ohms. The coupling capacitors, the probes in this case, transform the effective resistance to a higher value in parallel with **Ro**, thus reducing the effective resistance across the resonator to a loaded value, $\mathbf{R_L}$. This results in a loaded Q, $Q_L = \mathbf{R_L} / \mathbf{X_{Lo}}$ that is lower than the unloaded Q_U. Coupling is proportional to capacitance – a larger capacitor produces more coupling and loads the resonator more.

Next, the 3 dB bandwidth (half-power bandwidth) of the loaded resonator may be calculated[11]:

$$BW = \frac{Frequency}{Q_L}$$

Or we may measure the 3 dB bandwidth BW and then calculate Q_L. It is difficult to calculate the effective capacitance, inductance, and resistance of a quarter-wave resonator, but measurement of bandwidth is straightforward. From my measurements and those published by WA5VJB, I estimate the unloaded Q_U of the pipe-cap resonators as 600 to 1000. Pretty good!

Knowing the Q_U, we can make some estimates of loss. If a resonator is very lightly loaded, for very narrow bandwidth, so that **Ro** is not much larger than $\mathbf{R_L}$, then much of the power will be dissipated in **Ro** – resulting in high loss. With more loading, **Ro** becomes less significant and more of the power is transmitted. The loss of a resonator may then be calculated[12]:

$$\textbf{Insertion Loss} = \mathbf{20}\log\left(\frac{Q_U}{Q_U - Q_L}\right)\textbf{dB}$$

So for a Q_U around 1000, the bandwidth can be as narrow as perhaps 1% of the resonant frequency before loss becomes significant, since 1% bandwidth equates to $Q_L = 100$, which gives a resonator loss of just under 1 dB. Of course, this loss is in addition to circuit losses – a typical pipe-cap filter loss is 2 or 3 dB total for 1% bandwidth.

Probe Length

The difficulty with pipe-cap filters is finding the right probe length for a desired bandwidth. There is no simple way to estimate the length, and it appears to vary significantly with frequency and to be fairly critical.

I realized this the hard way, while trying to make filters for 2304 and 3456 MHz. I thought that making them a little longer than ones I had used at 5760 MHz would be fine, but the results were not. Tuning was extremely sharp, and the circuit had so much loss that I wondered if the MMIC amplifiers were defective and not amplifying. After spending far too much time troubleshooting, I began to suspect the pipe-cap probes.

Since my circuit was not conducive to controlled probe-length experiments, I turned instead to software, simulating the pipe caps using Ansoft **HFSS** software. Very short probes yielded sharp, lossy response curves, while long ones seemed rather broad. At each resonant frequency, or screw length, the best probe length was proportional to the screw length. Longer screw lengths, for lower frequencies, require much longer probes. I simulated enough data points to make a set of design curves for one-inch pipe caps so that I could predict my filter response. These curves have proven very useful and my circuits now work more predictably.

For future work, both for myself and others, I made similar curves for other common sizes: ¾ - inch, useful at 5760 MHz, and ½ - inch, for 10 GHz.

1” Pipe-Cap Filters

Longer probes increase the coupling to the resonator, lowering the loaded $\boldsymbol{Q}$, $\boldsymbol{Q_L}$, thus increasing the resonator bandwidth, as shown in Figure 5. Some other results are apparent – not only does the bandwidth increase, but the out-of-band rejection decreases, particularly above the resonant frequency. This may be due to direct coupling between the probes. With shorter probes, the filter gets much sharper, but the loss also increases.

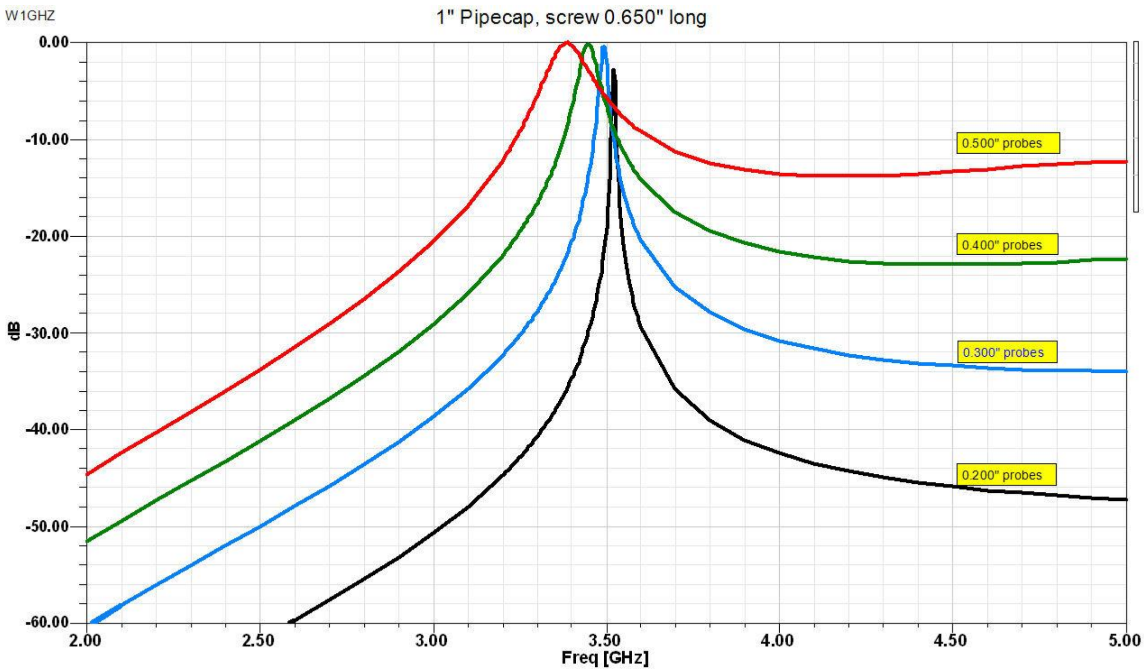


Figure 5. Pipe-cap bandwidth as a function of probe length

The curves in Figure 5 are at one tuning screw setting – the probe length only affects the resonant frequency by a small amount. If the resonant frequency is varied, by tuning the screw, the bandwidth for a given probe length increases with frequency, as shown in Figure 6. However, I have trouble using this curve as a design guide for probe length. If we instead plot bandwidth curves vs probe length for each screw setting, in Figure 7, then it is easier to estimate a good probe length for a desired frequency – just refer back to Figure 3 to estimate the resonant frequency corresponding to each screw length.

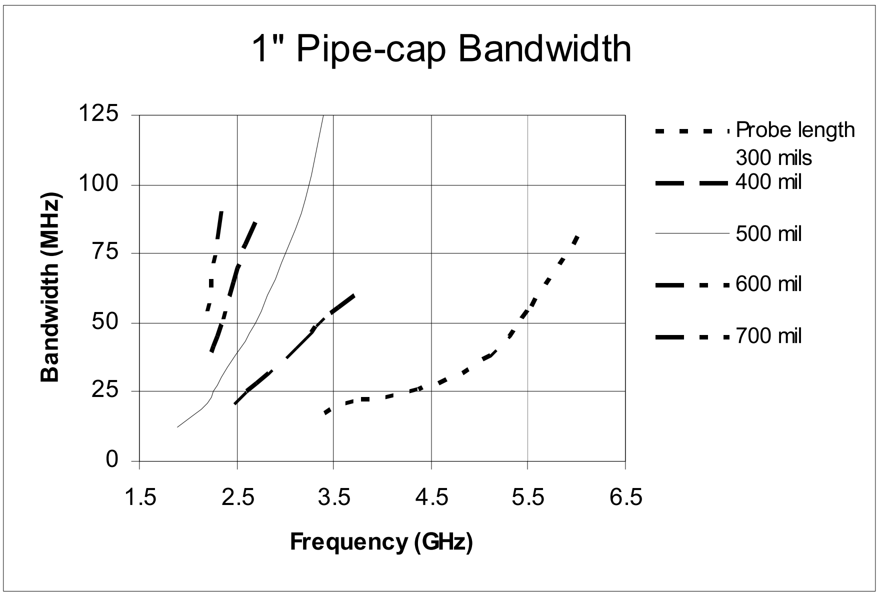


Figure 6

Loss is much harder to simulate, since the losses are not in the materials, but in the details. A threaded screw is a rough surface for RF, and rough surfaces increase loss. Even worse is the screw contact to the pipe cap – this is at the maximum current point of the resonator, where even small resistances add loss.

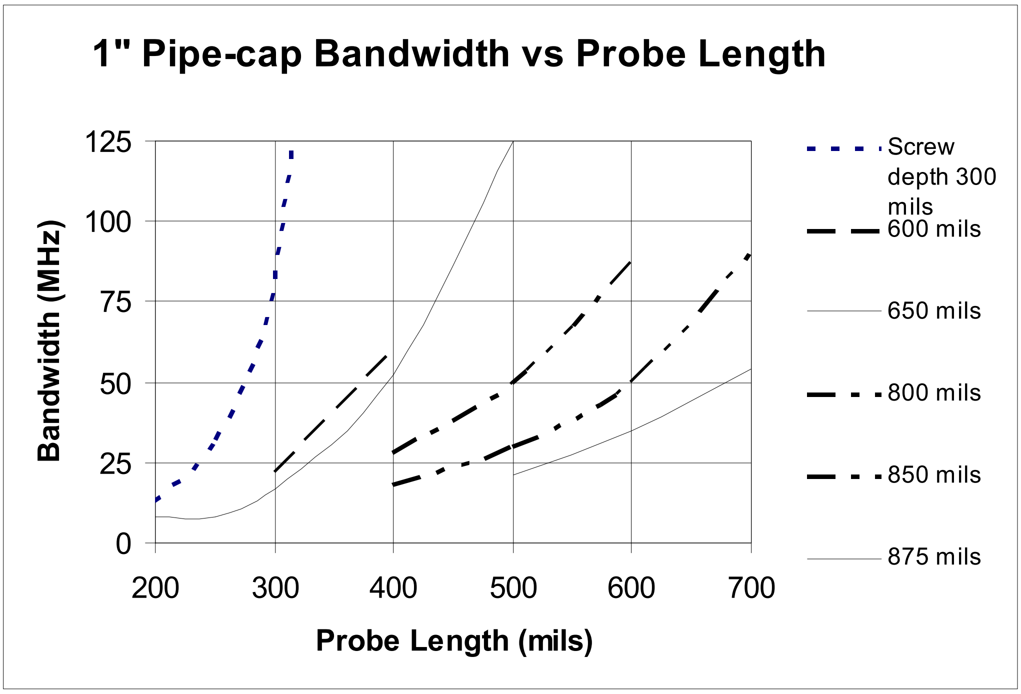


Figure 7

So losses are better characterized by measurement. Didier, KO4BB, made a suggestion on the WA1MBA microwave reflector that a pipe-cap filter could be held together by a C-clamp to allow quick adjustments. Since the rim of the pipe cap is in a high-impedance, low current area, contact resistance is not critical. I put together the test fixture shown in Figure 8 and made some measurements using my ancient HP-8410 Network Analyzer. No fancy computer corrections are used, so these numbers aren't precise.

Figure 8

The measured curves of bandwidth vs probe length for each screw setting, in Figure 9, show bandwidth increasing with probe length for longer probes, but flattening out with shorter probes. What is happening is that the equivalent resistance **Ro** due to losses is controlling the bandwidth, rather than the loading of the probes. Thus, the bandwidth remains constant but loss increases.

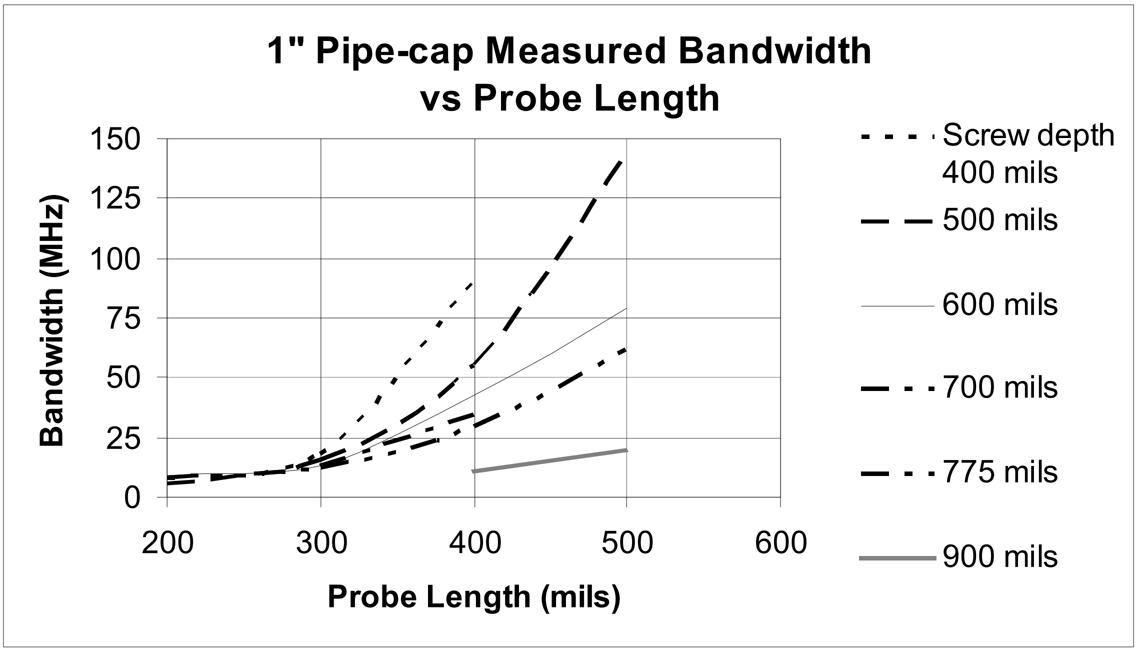


Figure 9

The measured losses are plotted in Figure 10. The test fixture seems to add around 1 dB of loss, probably because it is built on ordinary epoxy-fiberglass PC board, rather than good Teflon microwave board. We can see that the loss gets high as we approach the flat area of the curves in Figure 9.

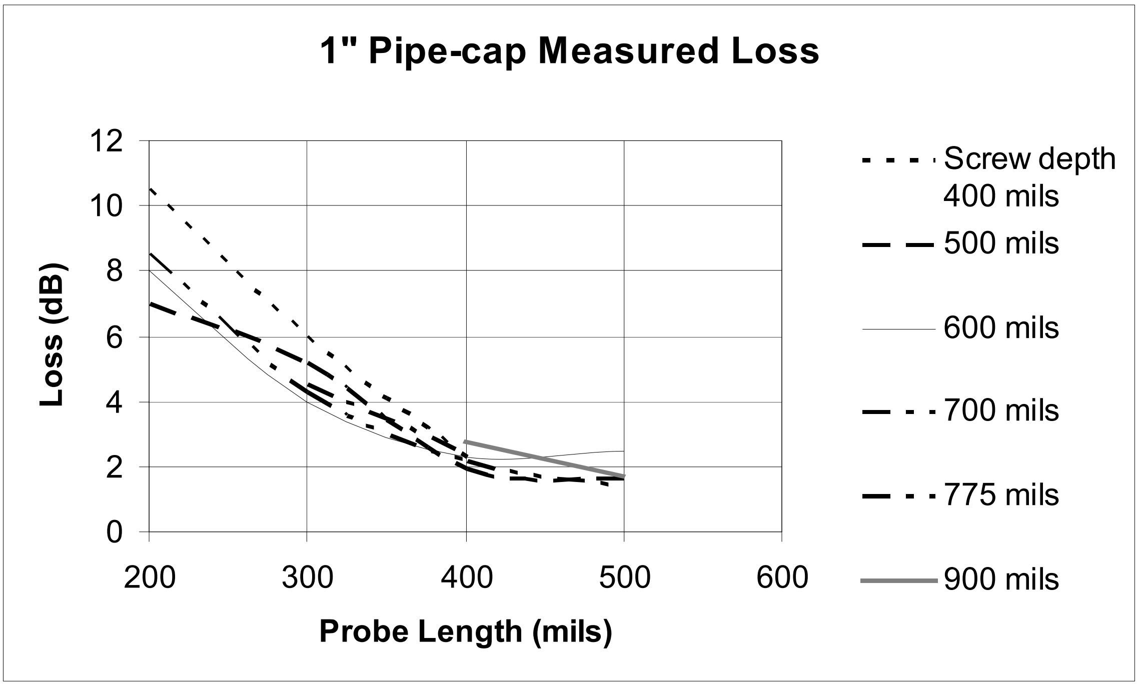


Figure 10

Plotting the loss vs the relative bandwidth of the resonator is much more illuminating. In Figure 11, we see that the loss increases rapidly for bandwidths less than 1% of the resonant frequency. This fits with our estimate of the unloaded $\boldsymbol{Q_U}$ around 1000. I also found that taller pipe caps have lower loss, so the $\boldsymbol{Q_U}$ is apparently higher. The better version, marked "NIBCO", are about 1.015" high overall, while the shorter ones are about 0.925" high. Obviously, the taller ones will tune to a lower frequency since they can accommodate a longer tuning screw.

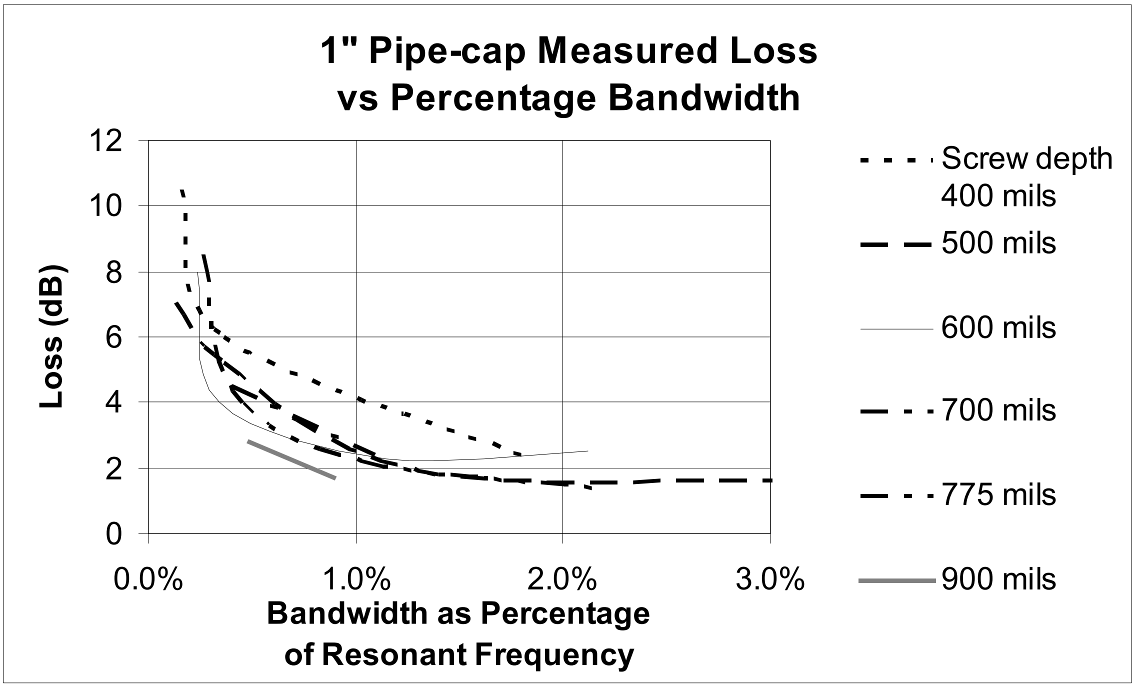


Figure 11

Since amateur operation is usually within a narrow frequency range, we usually want narrow filters with low loss. With pipe caps, we can make reasonably low loss filters with 3-dB bandwidths in the range of 0.5% to 2% of the resonant frequency – for instance, 17 to 80 MHz bandwidth at 3456 MHz.

While the 3-dB bandwidth is quite narrow, the skirts of a single resonator are not steep, so the out-of-band rejection, 20 or 30 dB down, can be much wider – see Figure 5. If a single resonator does not provide adequate rejection, multiple resonators may be cascaded. Direct connection will not work predictably, since the resonators will interact and the response will depend on the length of transmission line between them. However, we can isolate the resonators from each other and compensate for the loss at the same time by putting MMIC amplifiers between them. Then each resonator will see a reasonable termination at each end and behave predictably, and the total response will be the sum of the resonators and amplifiers.

One final note on probe length: all the curves above are for bare probes extending into the pipe cap from a PC board, like the "PCB input" in Figure 1. The results published by

WA5VJB used semi-rigid cable connections, like the "Coax input" in Figure 1, with the center conductor extending into the pipe cap as a probe and the Teflon insulator extending the whole length of the probe. The Teflon appears to increase the capacitive coupling, so that the response of these probes is similar to a longer bare probe.

1/2" Pipe-Cap Filters

These small pipe caps work well at 10 GHz, and Figure 3 shows that they can be tuned down to about 5 GHz. Curves for the half-inch pipe caps are shown in Figure 12, as a function of resonant frequency, and in Figure 13, as a function of probe length for each tuning screw position. In the latter plot, we can again see the bandwidth leveling off for short probe lengths, an indication of increasing loss. Like the one-inch version, it appears that the loss will increase for 3-dB bandwidths less than 1% of the resonant frequency.

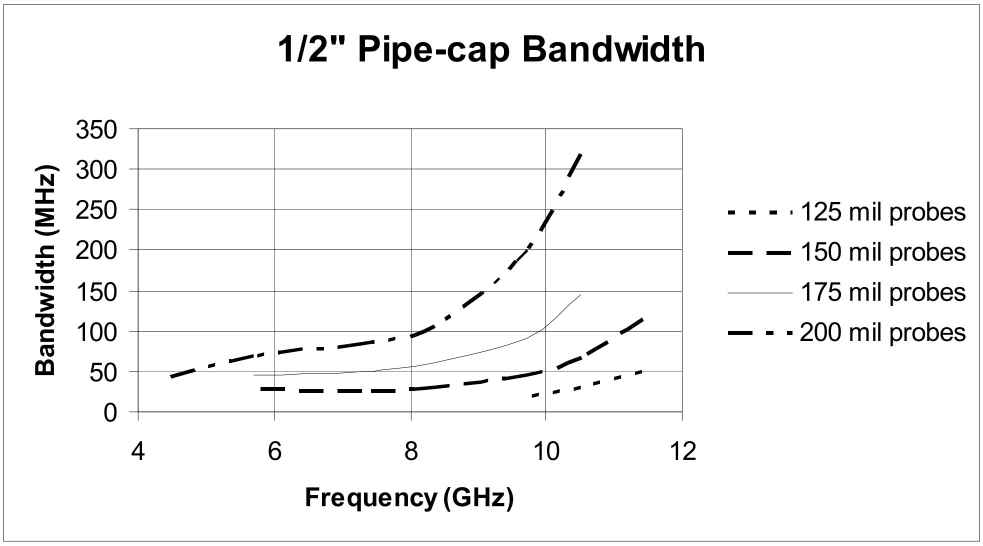


Figure 12

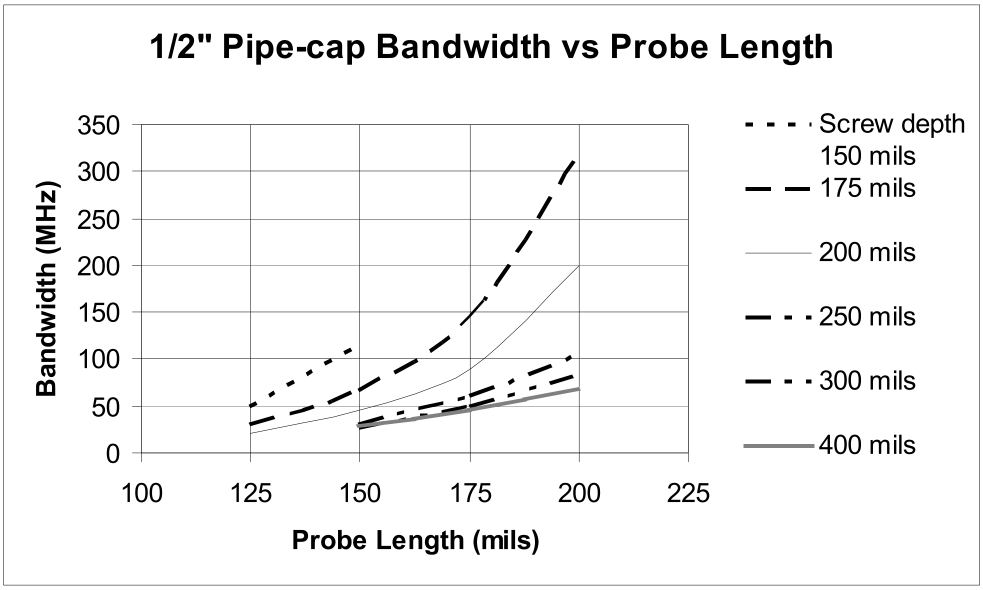


Figure 13

I did not make any measurements for ½ inch pipe-caps, but did scan the measured curves from my 1993 paper[3], in Figure 14. At 10.368 GHz, the compromise probe length is about 5/32"; shorter probes are lossy, and longer ones are not sharp enough. The difference between these three conditions is about 1/32 of an inch, which is about as close as I can control the length. For a 3 dB bandwidth around 1% of 10 GHz, a single resonator is not selective enough for good LO and image rejection, so multiple pipe-caps were needed. Since each pipe-cap resonator had more than 3 dB of loss at 10 GHz and good MMICs only have around 10 dB of gain, alternating pipe-cap resonators and MMIC amplifiers is a good combination.

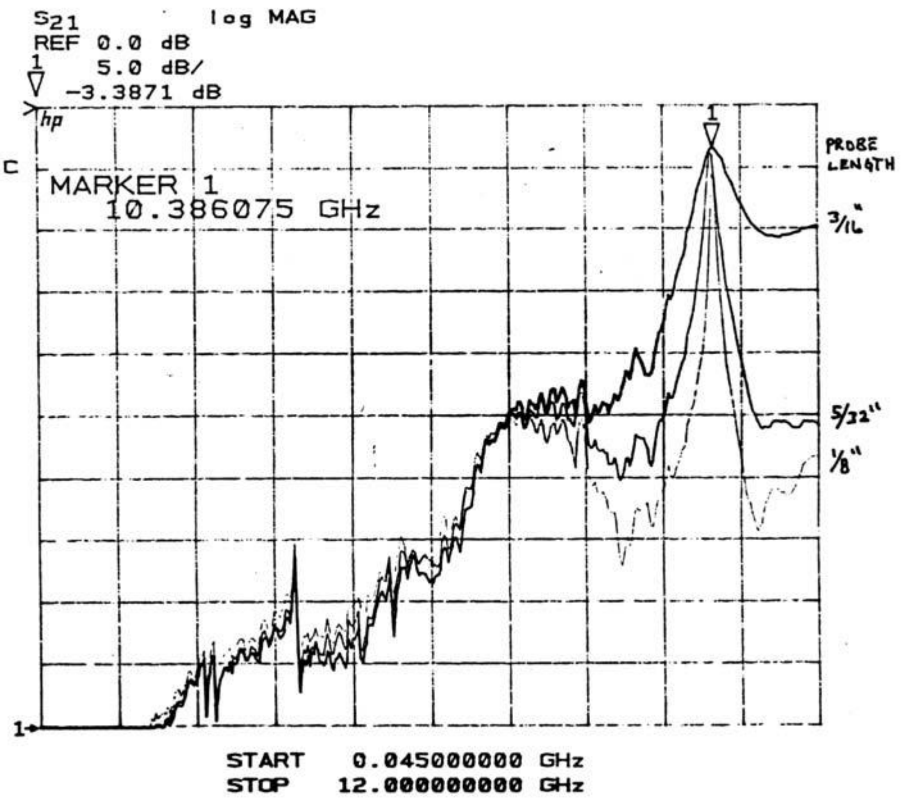


Figure 14. Measured response of 1/2" pipe-cap filter

3/4” Pipe-Cap Filters

Three-quarter inch pipe caps are ideal for 5760 MHz. I also used them at 3.3 GHz in the multiplier chain of the 10 GHz single-board transverter[7]. Curves for the ¾ -inch pipe caps are shown in Figure 15, as a function of resonant frequency, and in Figure 16, as a function of probe length for each tuning screw position. In the latter plot, we can again see the bandwidth leveling off for short probe lengths, an indication of increasing loss. Like the one-inch version, it appears that the loss will increase for 3-dB bandwidths less than 1% of the resonant frequency. While I can’t find records from measurements, I recall that the typical loss is lower than the ½ -inch version, probably similar to the one-inch version.

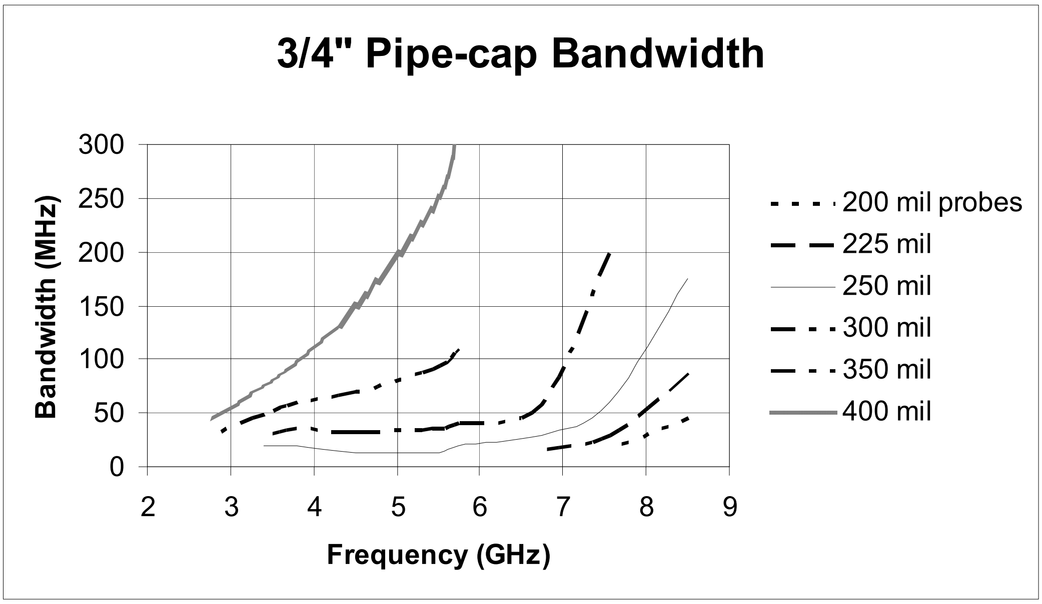


Figure 15

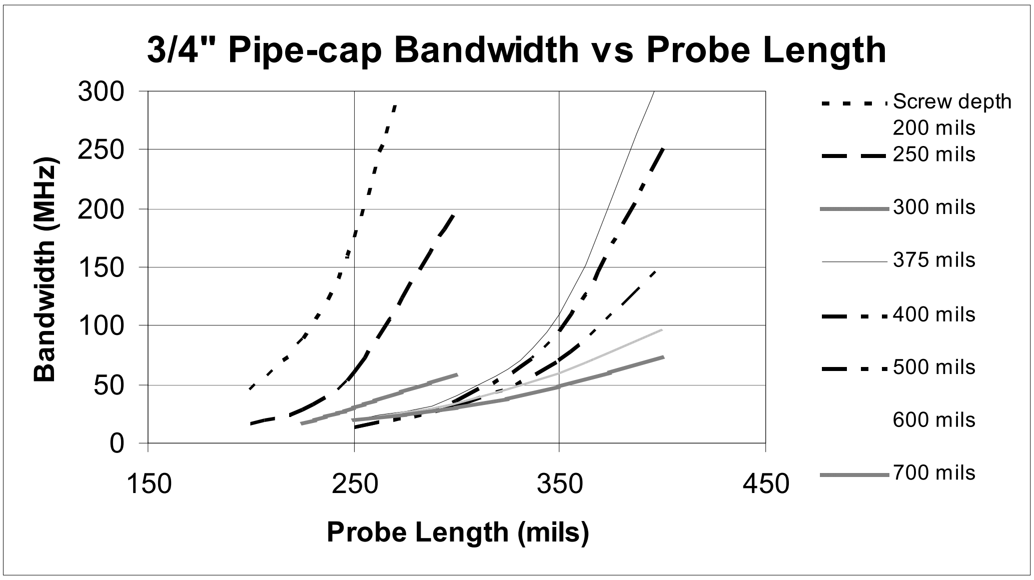


Figure 16

Larger Pipe-caps

Pipe-caps for larger diameter pipe are not significantly taller than the one-inch variety. Thus, they cannot accommodate much longer screws, so will not operate much lower in frequency. On a printed-circuit board, one would occupy significantly more area, which is hardly an advantage. The only potential advantage might be that the probes could be spaced farther apart, which might improve stopband attenuation.

Summary

Pipe-cap filters are simple and inexpensive microwave filters. The design curves here should help understanding and enable their use in homebrew projects. The curves are useful not just in the ham bands but for other frequencies, such as in multiplier strings or just interesting projects like receiving deep-space probes.

Table 1. Nominal Pipe Cap Dimensions

Size	Inner Diameter	Inside Height	Probe Spacing
1/2"	0.625"	0.565"	0.375"
3/4"	0.875"	0.880"	0.5"
1"	1.125"	0.920"	0.7"

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